

IMPROVED TURBO DECODER

Field of the Invention

The present invention relates generally to error-correction coding and, more particularly, to a decoder for concatenated codes, e.g., turbo codes.

Background of the Invention

Data signals, in particular those transmitted over a typically hostile RF interface, are susceptible to errors caused by interference. Various methods of error correction coding have been developed in order to minimize the adverse effects that a hostile interface has on the integrity of communicated data. This is also referred to as lowering the Bit Error Rate (BER), which is generally defined as the ratio of incorrectly received information bits to the total number of received information bits. Error correction coding generally involves representing digital data in ways designed to be robust with respect to bit errors. Error correction coding enables a communication system to recover original data from a signal that has been corrupted. Typically, the greater the expected BER of a particular communication link, the greater the complexity of the error correction coding necessary to recover the original data. In general, the greater the complexity of the error correction coding, the greater the inefficiency of the data communication. The greater inefficiency results from a reduction of the ratio of information bits to total bits communicated as the complexity of the error correction coding increases. The additional information introduced into the original body of data by error correction coding consumes spectrum bandwidth and processor cycles on both the transmitting and receiving ends of the communication.

In cases where the expected BER of a particular communication link is substantially higher than the acceptable BER, a concatenated set of error correcting codes may be applied to the data in order to lower the BER to acceptable levels. Concatenated

error correction coding refers to sequences of coding in which at least two encoding steps are performed on a data stream. Concatenated coding may be performed in series, where encoded data is subjected to further encoding, or in parallel where the original data is subjected to different encoding schemes to perform intermediate codes which are then further processed and combined into a serial stream.

Parallel and serial concatenated codes are sometimes decoded using iterative decoding algorithms. One commonly employed method of iterative decoding utilizes a single decoder processor where the decoder output metrics are fed back to the input of the decoder processor. Decoding is performed in an iterative fashion until the desired number of iterations have been performed. In order for the decoder processor to decode the encoded input data at the same rate as the input data is arriving, the decoder processor must process the encoded data at a rate faster than the rate of the incoming data by a factor at least equal to the number of iterations necessary. With this method of iterative decoding, the speed of the decoder processor becomes a significantly limiting factor in the system design.

Turbo codes are examples of parallel concatenated coding and are used as a technique of error correction in practical digital communications. The essence of the decoding technique of turbo codes is to produce soft decision outputs, i.e. different numerical values which describe the different reliability levels of the decoded symbols, which can be fed back to the start of the decoding process to improve the reliabilities of the symbols. This is known as the iterative decoding technique. Turbo decoding has been shown to perform close to the theoretical limit (Shannon limit) of error correction performance after 18 iterations - C. Beerou, A. Glavieux, and P. Thitimajshima, "Near Shannon Limit Error-Correcting Coding: Turbo Codes." In Proc. IEEE Int. Conf. Commun., Geneva, Switzerland, 1993, pp. 1064-1070. The Turbo Decoding algorithm is a very complex task as it takes up a large amount of computation time and consumes a lot of memory resources.

A turbo encoder is shown in figure 1 and comprises a pair of parallel-concatenated convolutional encoders (12, 13) separated by an interleaver (11), where the interleaver plays a role to shuffle (interleave) its input sequence in a pre-determined

order. It accepts an input binary $\{0,1\}$ sequence of a specified code block of size N symbols, and produces three types of encoded output for each symbol when the coding rate is $1/3$.

Referring to figure 2, a turbo decoder receives the encoded signals and uses all three types of signals when the coding rate is $1/3$ to reproduce the original bit sequence of the turbo encoder input. Two MAP decoders 21 and 24, associated with the convolutional encoders 12 and 13 respectively, perform the decoding calculations. In addition to an interleaver 22 to mirror the interleaver 11 of the encoding side, the turbo decoder also consists of a deinterleaver 23 to reconstruct the correct arrangement of the bit sequence to be fed back from 24 to 21. The decoded bits after the final iteration are hard decisions, i.e. output binary sequence $\{0,1\}$, obtained from 24.

A MAP decoder uses the BCJR algorithm - see C. Beerou, A. Glavieux, and P. Thitimajshima, "Near Shannon Limit Error-Correcting Coding: Turbo Codes." In Proc. IEEE Int. Conf. Commun., Geneva, Switzerland, 1993, pp. 1064-1070 - to compute the soft outputs, or likelihood. Using the received signals x , y and z , the algorithm computes three types of probabilities: α , β and λ .

In a sense, α represents the likelihood probability of a symbol changing from a state m' to another state m as the time interval progresses from t to $t+1$. The β probability, on the other hand, corresponds the likelihood probability of a symbol changing from a state m to m' from the time interval t to $t-1$. α and β are also known as *forward* and *backward* probabilities. The initial values for α and β are known because the states at the start and the end of the block L are set to zero in the turbo encoder. The λ probability fuses α and β together to obtain one measure of likelihood for each symbol. Then, the λ will be used to compute the output of the turbo decoder which will be either the soft decisions (feedback) or the hard decisions ($\{0,1\}$ bits).

These three probabilities must be computed sequentially, and normalized for each symbol. The computation sequences of α , β and λ is briefly shown in Figure 3. The state transitions in Beta and Alpha computation are shown in Figure 4. The eight

states correspond to the eight states of the constituent encoders in Turbo Encoder with 1/3 coding rate. There are two eight state constituent encoders, 12 and 13, in Turbo Encoder which follow the polynomials: $g_0(D) = 1+D^2+D^3$ and $g_1(D) = 1+D+D^3$ respectively. The $\text{Next}[m][0]$ and $\text{Next}[m][1]$ refer to next state as "0" and "1". The $\text{prev}[m][0]$ and $\text{prev}[m][1]$ refer to previous state as "0" and "1". The branch matrix computation of α and β will follow the state transitions in Figure 4.

As can be seen in the reference [Bahl et.al], the α and β are independent of each other, but λ is dependent on α and β . A complete algorithm requires that the α and β probabilities for all symbols L to be used to calculate λ .

According to the general SubLogMAP Algorithm of Turbo Decoder, the procedure of Turbo decode is (a) to calculate β values, (b) to calculate α values and (c) to calculate λ finally as shown in Figure 3. Figure 5 shows the overall structure for the calculations of β , where the β computation and normalization are performed whose results are fed back to the β computation paths as well as written into the β memory which will be read out on the next phase (α and λ computation). The details and critical paths of β computation and normalization paths are shown in Figure 6. Figure 10 shows the LSI architecture for the calculations of α . The details and critical paths of α computation are shown in Figure 12. There is a key operation, the normalization for β and α calculation to reduce the hardware amount. Normalization is needed to avoid the overflow of β and α computation. As shown in Figure 6 and 12, normalization process consists of (1) maximum values selection from the eight state values and (2) subtract of this maximum values from these eight state values, which will be fed back to the next computation. Because we are only interested in the maximum values of likelihood capabilities, this normalization is very effective to reduce the bit widths of the β and α computation data paths and various kinds of memories. Because the total calculation (β and α value computation and the normalization) is composed of fairly long critical paths as shown in Figure 6 for β calculation and Figure 12 for α calculation, the slower computation speed will be obtained. Figure 11 shows the overall structure for the calculations of λ . The details and critical paths of λ computation paths are also shown in Figure 12 (Shaded

operation in the figure). As can be seen in Figure 12, a lot of adders can be shared between the α and λ computation. There is also a long critical path from α value computation to LLR (Log-likelihood Ratio) computation for the calculations of λ .

The timing sequence of β computation is shown in the upper half portion (Beta Computation Stages Before Pipelining) of Figure 9 as an example. As can be seen in this Figure 9, each β computation and normalization is sequentially performed in one clock cycle, and the normalized β feedback is performed at the beginning of the next clock cycle. Similarly, each α computation and its normalization or λ computation and its LLR selection are sequentially performed in one clock cycle period. As shown in Figure 6 and Figure 12, the long critical path limits the speed of operating clock frequency. The calculation speed limitation of this architecture is caused by this longer clock cycle period time, in which the values of α and β are calculated.

As mentioned previously, the speed issue of turbo decoder implementation is the limitation of clock speed. The clock speed is decided by its cycle period in which the values of α and β are calculated. This is the critical path of the LSI implementation (or called maximum delay time of the calculation). There are two main operations (1) value calculation for α , β , and λ and (2) normalization for α and β , and LLR selection for λ in one clock cycle period to increase the critical path as shown in Figure 6, Figure 9 and Figure 12. This kind of sequential operations slow down the clock speed. Recently, as turbo coding is applied to real systems for higher data rate transmission, we need to employ faster turbo decoding while keeping the buffer storage requirement as small as possible.

Summary of the Invention

The present invention aims to provide a method and apparatus for iteratively decoding signals encoded with concatenated codes, including turbo codes.

In general terms, the present invention provides a recursive decoder having means for switching between normalised and non-normalised likelihood values or probability estimates (of received symbols) as feedback values for the next iteration of likelihood

values. For example in a MAP algorithm for decoding turbo encoded signal symbols, the decoder is arranged to switch between normalised and non-normalised values of the alpha and beta values. This could also be applied to other algorithms.

In prior art arrangements a normalisation function is implemented after the iterative calculation function in order to obtain normalized values of next state likelihood values which are then fed back to the calculation function for the next iteration. Normalization is needed to avoid the overflow of β and α computation. However this requires a long clock cycle for each iteration, which limits the clock speed available. The invention avoids some of the calculation time associated with normalising each state's likelihood values by bypassing the normalisation function in the feedback circuit for some states using the switch. For example, by feeding back only normalised values for the last state, the speed of calculating the final (hard) likelihood values is essentially halved. Meanwhile the normalised values for each state are still written to memory in the usual manner.

This increased speed of determining the likelihood values is particularly advantageous in modern wireless communications systems where error coding is essential, but where it must be accomplished quickly given the increasing adoption of high bandwidth wireless applications such as video phones and web-browsing.

In particular, in a first aspect the present invention provides a decoder for decoding encoded data, the decoder comprising:

- a processor having an input which receives probability estimates for a block of symbols, and which is arranged to calculate probability estimates for said symbols in a next iterative state;

- normalising means which normalises said next states estimates;

- a switch that receives both said normalised and said unnormalised next state estimates, the output of the switch being coupled to the input of the processor;

- wherein the switch is arranged to switch between the normalised and unnormalised next state estimates depending on the iterative state.

In another aspect the present invention provides a decoder for decoding encoded data, the decoder comprising:

a processor having an input which receives probability estimates for a block of symbols, and which is arranged to calculate probability estimates for said symbols in a next iterative state;

normalising means coupled to the processor which normalises said next states estimates;

wherein the decoder further comprises pipelining means between the processor and the normalising means for providing non-normalised next state estimates.

These non-normalised next state estimates can then be fed back into the processor input to calculate the next next state estimates. This architecture halves the usual critical path into before and after pipelining means halves. Because this critical signal propagation delay is halved, the clock speed can be doubled, and hence the overall processor speed for the decoder is increased.

Preferably the decoder further comprises switching means that receives both said normalised and said unnormalised next state estimates, the output of the switch being coupled to the input of the processor;

wherein the switch is arranged to switch between the normalised and unnormalised next state estimates depending on the iterative state.

In another aspect there is provided a processor for a decoder for decoding encoded data, the processor comprising:

means for calculating probability estimates for a block of symbols said symbols in a next iterative state;

pipelining means which receives the next state estimates; and

normalising means which normalises said next states estimates.

As this part of the processor represents the critical path, by splitting this path with pipelining means, the clock speed can be increased and hence the overall decoder

performance is enhanced, at the relatively modest hardware cost of adding some pipeline registers between the calculating means and the normalising means.

Brief Description of the Drawings

Embodiments of the invention will now be described with reference to the following drawings, by way of example only and without intending to be limiting, in which:

Figure 1 is a schematic of a basic turbo code encoder;

Figure 2 is a schematic of a basic turbo code decoder;

Figure 3 is shows a sequence schematic of alpha, beta and lambda calculations;

Figure 4 shows state transitions in alpha and beta computation;

Figure 5 shows a prior art beta computation block diagram;

Figure 6 shows prior art beta computation and critical path diagram;

Figure 7 shows beta computation and critical path diagram according to an embodiment of the invention;

Figure 8 shows a beta computation block diagram according to an embodiment of the invention;

Figure 9 shows the timing diagram of the stages of beta computation for both prior art and an embodiment of the invention;

Figure 10 shows a prior art alpha computation block diagram;

Figure 11 shows a prior art lambda computation block diagram;

Figure 12 shows prior art alpha and lambda computation and critical path diagram;

Figure 13 shows alpha and lambda computation and critical path diagram according to an embodiment of the invention;

Figure 14 shows a alpha computation block diagram according to an embodiment of the invention;

Figure 15 shows a lambda computation block diagram according to an embodiment of the invention;

Figure 16 shows BER v SNR simulation results for a prior art decoder and an embodiment of the invention (Block length = 3856 bits); and

Figure 17 shows BER v SNR simulation results for a prior art decoder and an embodiment of the invention (Block length = 5114 bits).

Detailed Description

Referring to Figure 6, the critical paths of β computation data path and normalization data path are nearly equal. Actual logic synthesis results show that they have almost the same propagation delay. Similarly, looking at Figure 12, the critical paths of α computation data path and its normalization paths, or the critical paths of λ computation data path and its LLR selection path are nearly equal. A first embodiment provides that we can divide these long critical paths into two pipeline stages.

Figure 7 and Figure 8 show the new architecture of the β calculation for the proposed implementation. As can be seen in Figure 7, the pipeline registers are inserted between the β computation and its normalization, which means the calculation of β is finished in two clock cycles instead of one cycle as previously shown in the upper half portion (Beta Computation Stages before Pipelining) of Figure 9. One stage is assigned for value computation and another is for the normalization. Because the

critical paths in β computation and those in normalizer are equally balanced as described above, the clock speed will be doubled to improve the system performance. The clock speed can be doubled because the propagation delay is halved, but the calculation and the normalisation are still required, Their processing is pipelined. The splitting the critical path and/or doubling the clock speed speeds up the whole system performance with the similar hardware architecture. It means the new architecture has more powerful processing capabilities which is very important for Turbo Decoder, but without a significant increase hardware complexity. In order to reduce the latency from feedback loop, we have added another feedback loop from the unnormalized β values. This feedback selection is performed by MUX (multiplexer) in Figure 8 to optionally choose the unnormalized β values ($\text{BetaU}[t][0]$, $\text{BetaU}[t][1]$, ..., $\text{BetaU}[t][7]$) or normalized β values ($\text{beta}[t][0]$, $\text{beta}[t][1]$, ..., $\text{beta}[t][7]$).

Because the normalized feedback is not performed for every β computation, we need to increase the bit width of the β computation data paths. Increasing the bit width added a little more hardware such as the registers and adders bit width. However this increases the system performance with high speed computation, with only a small amount of hardware added. However because the normalization is performed for every β value to be stored to the β memory, it is not necessary to widen the β memory bit width.

Preferably the feedback ratio of normalized values to the unnormalized values is set to 1/8, i.e., if a normalized feedback cycle is inserted after every eight unnormalized feedback cycles. According to simulation results, only two-bit increase of the computation data path is required. Whilst normalization is needed to avoid the overflow of β and α computation, system simulation shows that the performance is not affected (see Figure 16 and 17).

The lower half portion of Figure 9 provides the detailed description of the timing sequence for this proposal for β calculation. The implementation architecture for original beta calculation is divided into two stages pipeline. The normalized feedback frequency is reduced to one time per every eight β value's computation. That's to use

the unnormalized feedback value for next β value computation for first seven β value computations, and just to use the normalized value for the last β value computation, for every eight actual calculations. That means every eight calculations, there is an idle or no-operation cycle (invalidated pipeline cycle) in order to perform the β value computation with the normalized feedback for the last β calculation. The procedure of β calculating is pipelined to reduce the length of critical path into the half of the previous procedure. The speed of operating clock is 2 times faster than the previous design, which can be seen from the Figure 9. The total throughput of β computation, therefore, is increased about double.

A similar implementation is applied to the α and λ computation paths. Figure 13, 14 and 15 show the pipelined structure of the α and λ computation paths, where the shaded operators are showing the λ computation path. The pipeline registers are inserted between the α computation and its normalization path, and also inserted between the λ computation and LLR selection paths as shown in the Figure 13. The unnormalized α feedback is performed as shown in Figure 14 by implementing MUX (multiplexer) to optionally choose the unnormalized α values ($\text{AlphaU}[t][0]$, $\text{AlphaU}[t][1]$, ..., $\text{AlphaU}[t][7]$) or normalized α values ($\text{alpha}[t][0]$, $\text{alpha}[t][1]$, ..., $\text{alpha}[t][7]$).

Because there is no feedback loop is needed for the λ computation path, we can divide this path into two stages at any arbitrary portion of the λ computation. As can be seen in Figure 13, the λ computation path is very similar with the β or α computation paths, it is suitable to insert the pipeline registers between the λ computation path and LLR selection path.

The detailed description of the timing sequence for the previous design and this proposal for α calculation is same as the one of β calculation, which is shown in Figure 9. The implementation architecture for original α calculation is modified as two stages pipeline. The normalization feedback frequency is reduced to one time per every eight α value's computation. That's to use the unnormalized feedback value for next α value computation for first seven α value computations, and just to use the normalized value for the last α value computation, for every eight actual calculations.

That means every eight calculations, there is an idle cycle in order to perform the α value computation with the normalized feedback for the last α calculation. The procedure of α calculating is pipelined to reduce the length of critical path into the half of the previous procedure. The speed of operating clock is 2 times faster than the previous design, which can be also seen from the Figure 9.

From the above description and the architectures diagrams in Figure 5, 6, 7, 8 and 9, the processing speed can be improved by two time faster compared with the implementation of the prior art. This is achieved by using the embodiment of pipeline computation implementation architecture and reduced normalization feedback computation for the values of β computation. We can save a lot of hardware resources (adders, max, and registers) by enabling the resource sharing between the Beta and Alpha computation to reduce the hardware amount. Beta and Alpha computations are timing sharing to use the same hardware module by timing control switch. The embodiment uses the same minimum memory storage of the prior art.

Furthermore, the proposed implementation will not have any effect on the performance of the decoder because the calculations of the probabilities are the same as the ones used in the prior art. Figure 16 and Figure 17 show the BER performance simulation comparison between the original normalization scheme (normalization feedback for every calculation) and the new normalization scheme for block bit length 3856 and 5114.

The various features of the described embodiments of the invention may be freely combined. Alterations and modifications as would be obvious to those skilled in the art are intended to be incorporated within the scope hereof.